GEC PLESSEY
SEMICONDUCTORS

3055-1.0

SL486

INFRA RED REMOTE CONTROL PREAMPLIFIER

The SL486 is a high gain preamplifier designed to form an interface between an infra-red receiving diode and the digital input of remote control receiving circuits. The device contains two other circuit elements. one to provide a stretched output pulse facility and a voltage regulator to allow operation from a wide range of supplies.

FEATURES

- Fast Acting AGC Improves Operation in Noisy Environments
- Differential Inputs Reduce Noise Pick-up and Improve Stability
- Gyrator Circuit Allows Operation in Environments with High Brightness Background Light Levels
- Output Pulse Stretcher for use with Microprocessor Decoders
- On-Chip Stabiliser Allows Operation with a Wide Range of Supply Voltages
- Low Noise Output

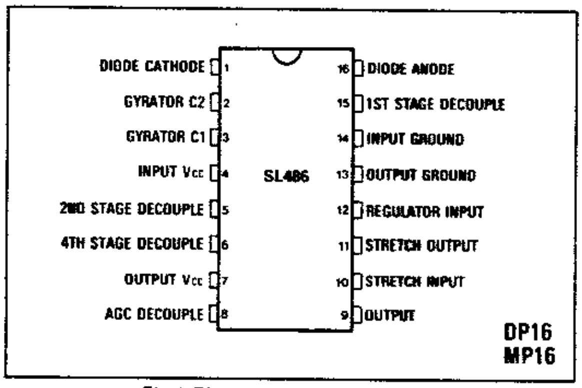


Fig.1 Pin connections (top view)

ABSOLUTE MAXIMUM RATINGS

Supply voltage (V Pins 4 & 7)	+10V wrt V Pins 13 & 14
Regulator input voltage (V Pin 12)	-20V wrt V Pin 7
Output current	5mA
Stretch output current	5mA
Operating temperature range	0°C to +70°C
Storage temperature	-55°C to +125°C

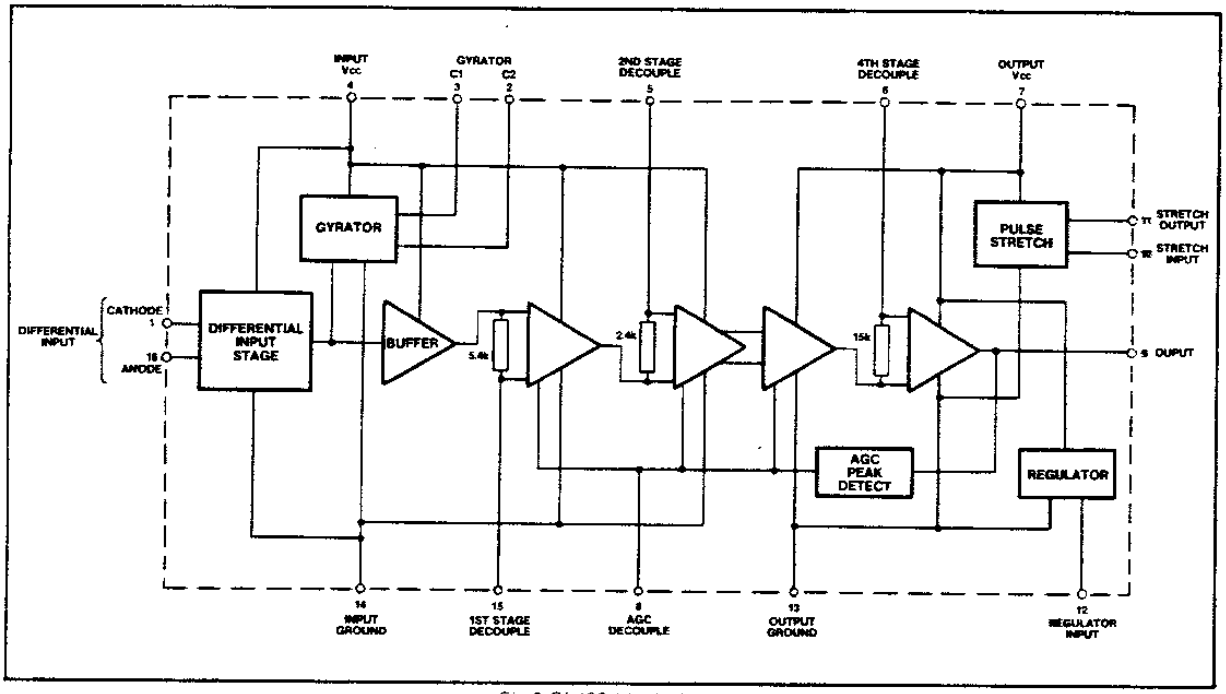


Fig.2 SL486 block diagram

ELECTRICAL CHARACTERISTICS

Test conditions (unless otherwise stated):
T_{amb} = 25°C, V_{CC} = 4.5V to 7.0V

Characteristic	Pin	Value			Unit	Conditions
		Min.	Typ.	Max.		
Supply current (See Note 1)	4,7		6.5	9.0	mA	V_{CC} = 5.0V, I_{DIODE} = 1.0μA } Pins 13 & 14 ground
	4	3.5+3xI_D	4.2+3xI_D	5+3xI_D	mA	V_{CC} = 4.5V, I_{DIODE} ≤ 1.5mA } Pins 13 & 14 ground
	4,7		8.5	10	mA	V_{CC} = 18V, I_{DIODE} = 1.0μA Pin 12 ground
Low voltage supply (external)	4,7(+ve), 13,14(-ve)	4.5		9.5	V	Input and output V_{CC} commoned, input and output ground commoned
High voltage supply (external)	4,7(+ve), 12(-ve)	8.4		18.0	V	Input and output V_{CC} commoned, input and output ground at internal regulated voltage
Internal regulated voltage	13(wrt 7)	5.9	6.2	6.5	-V	V Pin 7(+) to V Pin 12(-) = +16V
Voltage between input and output V_{CC}	4,7			1.5	V	At room temperature
				1.1	V	At 70°C
Minimum sensitivity of differential input	1,16	9.0		2.3	nA	I_{DIODE} = 1.0μA
		74.0		18.5	nA	I_{DIODE} = 100μA
		168.0		42.0	nA	I_{DIODE} = 0.5mA
Common mode rejection	1,16		35.0		dB	
Maximum signal input	1,16	3.0	4.0		mA(peak)	
AGC range			68.0		dB	
Output and stretch output pull-up resistance (internal)	9,11		55.0		kΩ	At 25°C
Stretch output pulse width (T_P)	11		2.4		ms	Capacitance Pin 9 to Pin 10 = 10nF; $T_P \simeq -R_X C \ln \left\{\frac{1.5}{V_{CC}}\right\}$,
T co-efficient on Rx			0.7		%/°C	Where Rx = 200kΩ ± 25% (internal resistance)
Output low	9			Output ground +0.35	V	0.2mA Sink, max.
Output high	9	Output V_{CC} -0.5			V	5μA Source
Stretch output low	11			Output ground +0.5	V	1.6mA Sink, max.
Stretch output high	11	Output V_{CC} -0.1			V	Output open circuit 5μA Source
Supply rejection, input V_{CC}	4		1.5		V(peak)	Ripple amplitude at 100Hz, Pin 12 ground
			0.8		V(peak)	Ripple amplitude at 100Hz, Pins 13 & 14 ground

NOTE
1. I_D = I_{DIODE} = IR diode forward current

APPLICATION NOTES - REFER TO FIGURE 4

Diode Anode and Cathode (Pins 1 and 16) The infra-red receiving diode is connected between pins 1 and 16. The input circuit is configured so as to reject signals common to both pins. This improves the stability of the device, and greatly reduces the sensitivity to radiated electrical noise. The diode is reverse biased by a nominal 0.65V.

Gyrator C2 and C1 (Pins 2 and 3) The decoupling, provided by gyrator C2 and C1, rolls off the gain of the feedback loop which balances the DC component of the infra-red diode current. The values of C2 and C1 are chosen to produce a low frequency cut-off characteristic below a nominal 2kHz. Hence, the gyrator produces approximately 20dB rejection at 100Hz.

The gyrator consists of two feedback loops operating in tandem. Only one feedback path is functional when the DC component of the diode current is less than 200μA. This loop is decoupled by gyrator C2. For diode currents between 200μA and 1.5mA the second control loop is operative, and this is decoupled by gyrator C1.

The decoupling capacitors, gyrator C2 and C1, must be connected between pins 2 and 3, to pin 4. The series impedance of C2 and C1 should be kept to a minimum.

First Stage Decouple (Pin 15) The capacitor on pin 15 decouples the signal from the non-inverting input of the first difference amplifier (see also Figure 2). The capacitance of 15nF is chosen to produce a 2kHz low frequency roll-off.

The capacitor must be connected between pins 15 and 14 (the input ground).

Second Stage Decouple (Pin 5) The capacitor on pin 5 decouples the signal from the non-inverting input of the second difference amplifier. The capacitance of 33nF is chosen to produce a 2kHz low frequency roll-off. The capacitor must be connected between pins 5 and 4 (the input Vcc).

Fourth Stage Decouple (Pin 6) The capacitor on pin 6 decouples the signal from the non-inverting input of the fourth difference amplifier. The capacitance of 4.7nF is chosen to produce a 2kHz low frequency roll-off. The capacitor must be connected between pins 6 and 7 (the output Vcc).

AGC Decouple/Delay Adjust (Pin 8) The output of the fourth difference amplifier is followed by a peak detector, which is used to provide an AGC control level. This produces a current source which is limited to 10mA at pin 8. The AGC decouple capacitor (C5 normally 150nF) filters the pulsed input, and the resultant level controls the gain of the first three difference amplifiers.

The AGC control level exhibits a fast attack/slow decay characteristic. Immediately infra-red pulses are detected, the gain will be reduced, so that any weaker noise pulses that are also received will not be seen at the output. Thus, provided the infra-red pulses are the most intense, it is possible to receive data in noisy environments. The slow decay keeps the AGC level intact during data reception, and produces a delay before any received noise may become present at the output, when transmission ceases.

Output (Pin 9) The output will be low, pulsing high with a source impedance of a nominal 55kΩ, for a received infra-red pulse. It is a linear amplification of the input and swings between output ground and output Vcc.

Stretch Input and Stretch Output (Pins 10 and 11) A typical infra-red PPM system transmits very narrow pulses. The duration of these pulses is typically 15μs, so in order to utilise a microprocessor based decoder system it is necessary to lengthen the received pulse. This stretched output can be obtained from pin 11 when a capacitor is connected between pins 9 and 10.

The width of the pulse is determined by the value of this coupling capacitor (C8 in Figure 3) and is given by:

$$T_P = -R_X C_8 \ln \left\{ \frac{1.5}{(V_4 - V_{13})} \right\}$$

where T_P = pulse width in ms
R_X = 200kΩ (see electrical characteristics)
C_8 = coupling capacitance
and $(V_4 - V_{13})$ = potential between input Vcc and ground (pins 13 and 14)

The stretch output is normally high pulsing low for a received infra-red pulse, and swings between output Vcc and output ground.

Regulator Input (Pin 12) The device can be operated with supplies of between 4.5V and 9.0V connected between input/output ground (pins 14 and 13) and input and output Vcc (pins 4 and 7) as shown in Figure 3.

The device can be operated with supplies in excess of 9.0V by utilising the on-chip regulator. In this case connections are made between output Vcc (pin 7) and the regulator input (pin 12) as shown in Figure 4. A supply voltage of between 9.0V and 18V will then cause the output ground to be regulated at a level nominally 6.4V below the output Vcc (pin 7).

The regulator will, however, lose control with a potential difference of less than 9.0V. Below this level the voltage on pin 13 will track nominally 1.5V above the level of pin 12.

When the regulator is not used (low voltage operation), pin 12 must be shorted to output ground (pin 13).

OPERATING NOTES - REFER TO FIGURES 3 AND 4

Gyrator C1 (Pin 3) If the environment in which the device is operating, limits the background light such that the DC component of the diode current has a maximum of 200μA, it may be desirable to omit (see Figure 3) the more bulky and costly 68μF capacitor, gyrator C1 shown in Figure 4. In this case pin 3 can be left open circuit. The resultant application will then have a characteristic of greatly reduced gain when the ambient light causes the DC current to rise above this threshold.

The 68μF capacitor can alternatively be replaced by a resistor. The outcome of this is to further reduce the gain in ambient light levels above the 200μA threshold. Below this threshold the overall gain is slightly enhanced as the light level approaches the threshold value. If chosen this resistance should lie between 10kΩ and 200kΩ.

Noise Immunity The stretch output can also be used as a means of improving performance relating to a receiver system, over and above its main purpose of providing a stretched output facility. Including C8 (Figure 4) causes the output pulses (from pin 9) to be subjected to the stretch input threshold. Thus any noise pulses from pin 9 that are below this threshold will not be seen at the stretch output (pin 11).

A further improvement can be made, utilising this stretch input threshold by including some additional filtering of the output (C10 in Figure 4). This can be adjusted in value (typically 100pF) to reduce some of the noise pulses that otherwise cross the threshold, to a level below the threshold.

It must be noted that the stretch output logic sense is inverse (for microprocessor applications) from that of the output (pin 9), and the cost of re-inversion may be deemed uneconomical for the improvements gained.

Screening Use of screening for the device, and associated components, improves the performance and immunity to externally radiated noise. The screening method used must protect the sensitive front-end of the device; provided that the diode, pin 1, pin 16, C2 (pin 2) and the first stage decouple (pin 15) are screened, it may be found that for the application considered, the remaining circuitry need not be so protected.

In applications where externally radiated noise is minimal, it may be possible to reduce any screening to pins 1 and 16, and the diode connections, only. In some instances, no screening may be necessary, but this largely depends on the level of radiated noise, the decoupling/filtering employed and the receivers decoding technique.

Decoupling Typical decoupling arrangements for use with or without the regulator, are given in Figures 4 and 3 respectively. When using the regulator, further improvements in high frequency supply rejection are possible by the inclusion of R2. The value can be chosen so as to keep the pin 12 end of R2 within the -9.0 to -18V (w.r.t. pin 7) specified voltage range. For example if using the 920 series remote control receivers, on a supply of 16V, a typical value for R2 would be 200Ω.

Note that the regulator is a low impedance point between pins 12 and 13. C7 thus maintains a low impedance path between pins 4 and 12 at high frequencies.

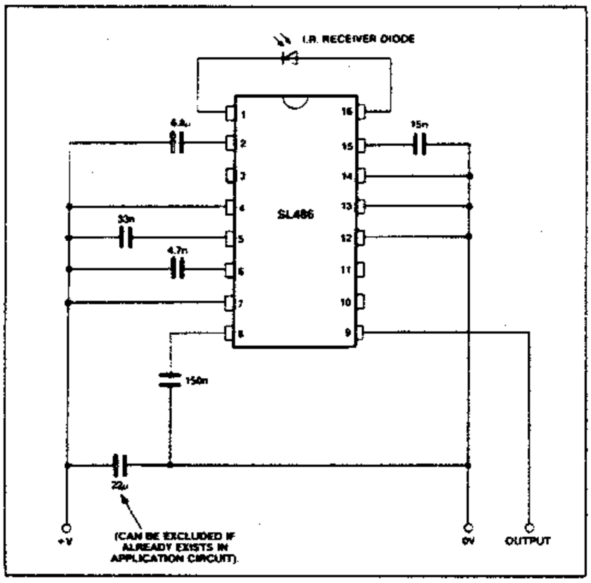


Fig.3 Circuit diagram of minimum component application (showing low voltage operation)

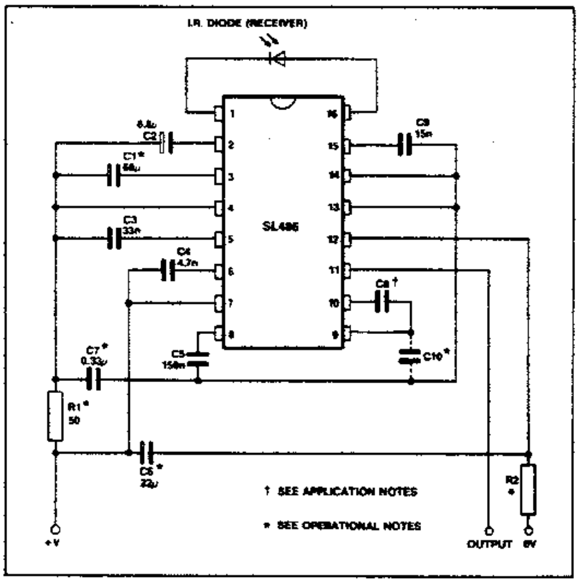
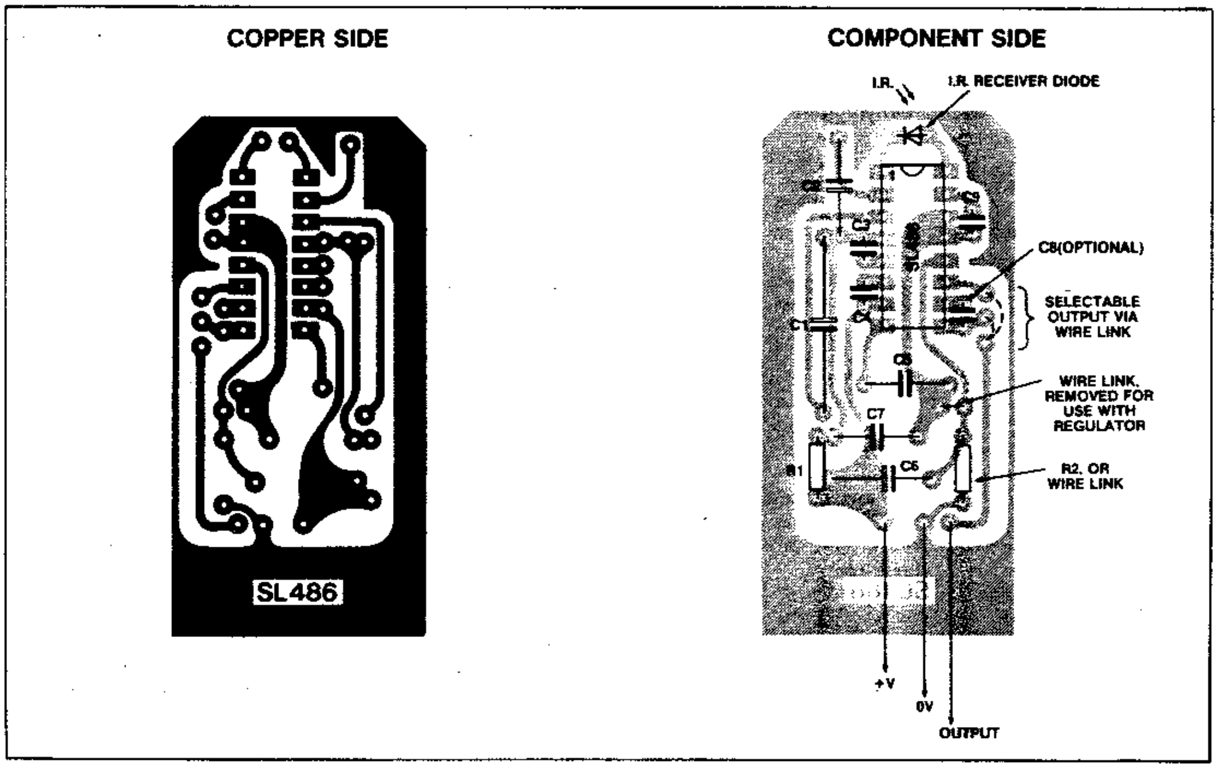


Fig.4 SL486 application diagram showing all optional circuitry (Note: Supply decoupling and connections for use of voltage regulator; also pulse stretched output)



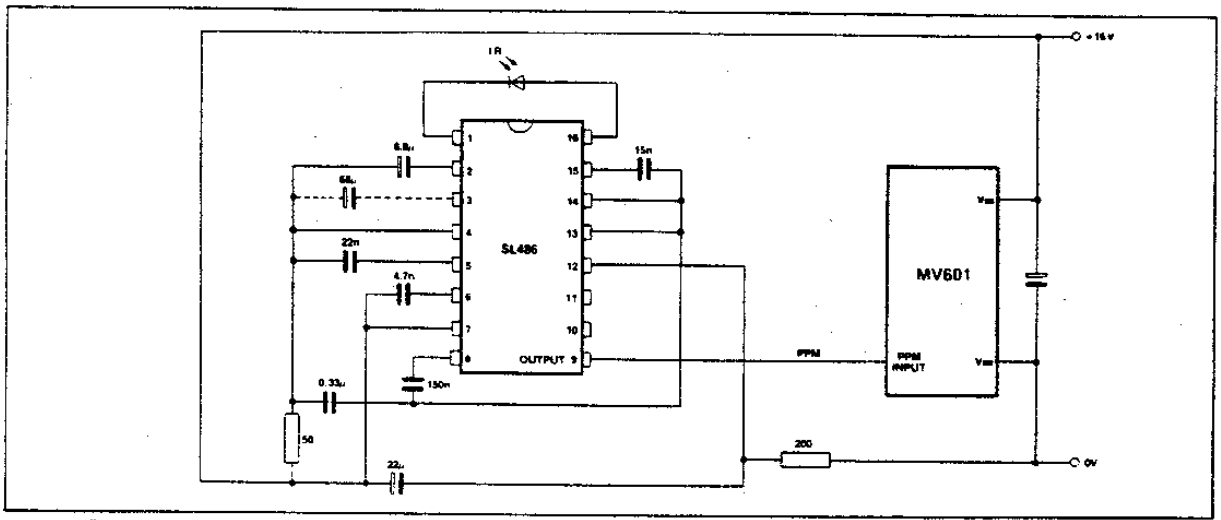


Fig.6 Application diagram for use with the MV601 remote control receiver, utilising on-chip supply stabiliser

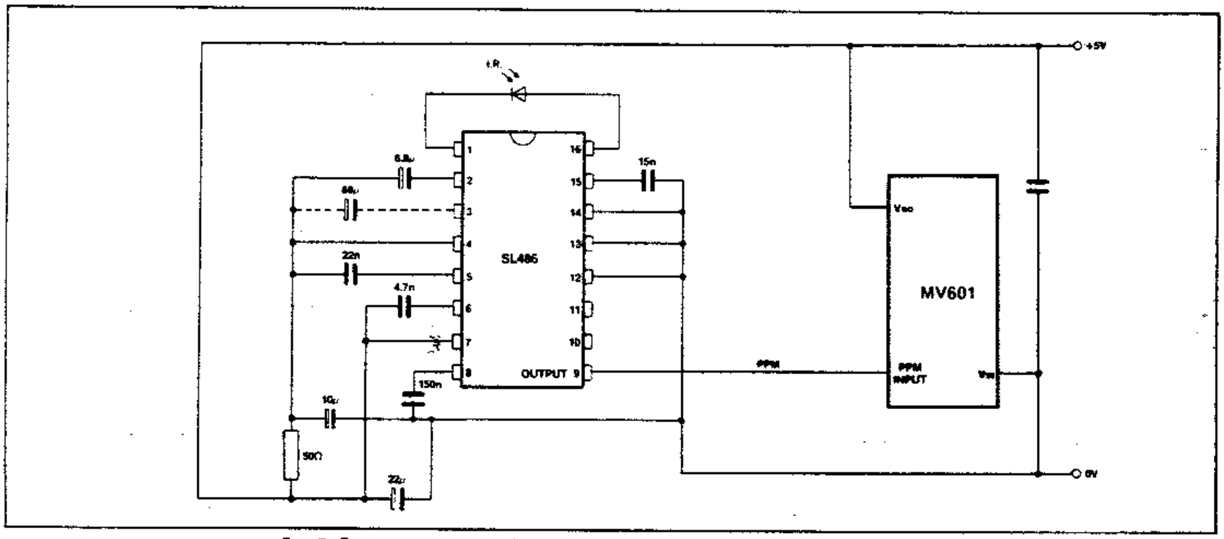


Fig.7 Circuit diagram of interface with MV601 remote control receiver

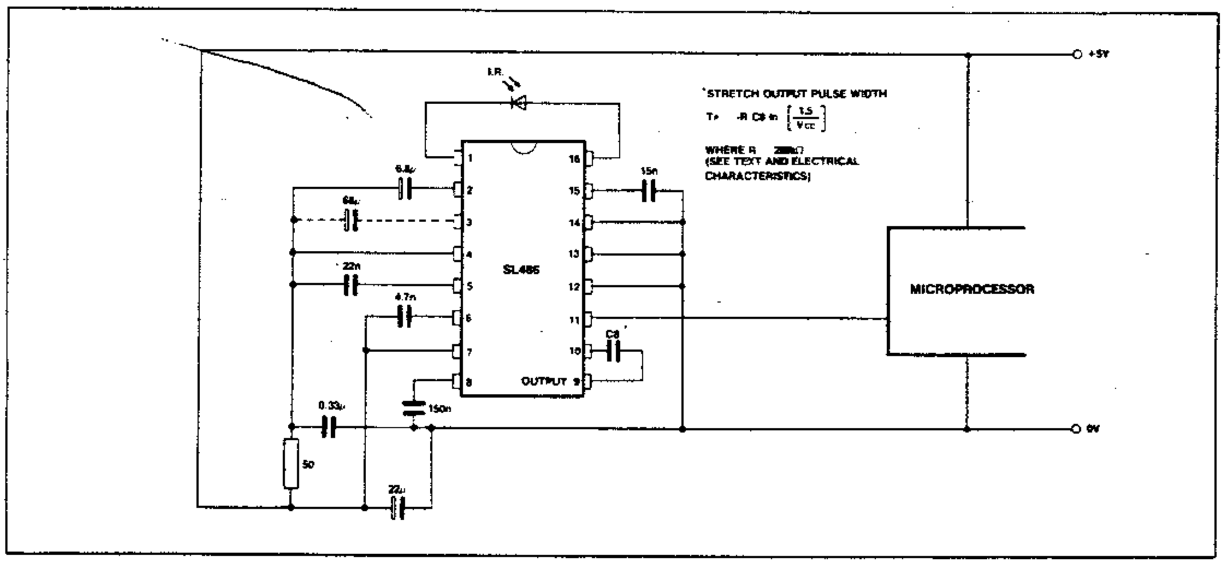


Fig.8 Circuit diagram of microprocessor interface, utilising on-chip pulse stretching facility